

IS32LT3953

CONSTANT-CURRENT 3-AMPERE PWM DIMMABLE BUCK REGULATOR LED DRIVER WITH FAULT PROTECTION

Preliminary Information
January 2018

GENERAL DESCRIPTION

The IS32LT3953 is a DC-to-DC switching converter, which integrate an N-channel MOSFET to operate in a buck configuration. The device supply a wide input voltage between 4.5V and 40V and provides a constant current of up to 3A for driving a single LED or multiple series connected LEDs.

The external resistor, R_{SET} , is used to adjust LED output current, which allowing the output voltage to be automatically adjusted for a variety of LED configurations.

The IS32LT3953 operates in a fixed frequency mode during switching. There is an external resistor connected between the VCC and TON pins used to configure the on-time (switching frequency). The switching frequency is dithered for spread spectrum feature to spread the electromagnetic emitting energy into a wider frequency band. It is helpful to optimize the EMI performance.

A logic input PWM signal to the enable (EN) pin is applied to adjust the LED current. The brightness of LED is proportional to the duty cycle of the PWM signal.

True average output current operation is achieved with fast transient response by using cycle-by-cycle, controlled on-time method.

IS32LT3953 is available in an SOP-8-EP package with an exposed pad for enhanced thermal dissipation. It operates from 4.5V to 40V over the temperature range of -40°C to $+125^{\circ}\text{C}$.

FEATURES

- Wide input voltage supply from 4.5V to 40V
- True average output current control
- 3A maximum output over operating temperature range
- Cycle-by-cycle current limit
- Integrated high-side MOSFET switch
- Dimming via direct logic input or power supply voltage
- Internal control loop compensation
- Under-voltage lockout (UVLO) and thermal shutdown protection
- $2\mu\text{A}$ low power shutdown
- Spread spectrum to optimize EMI
- Robust fault protection:
 - Pin-to-GND short
 - Component open/short faults
 - Adjacent pin-to-pin short
 - LED open/short
- AEC-Q100 qualification in progress

APPLICATIONS

- Automotive and avionic lighting
- Dimmable interior lights
- Daytime running lights
- Turn/stop lights
- Front and rear fog lights
- Map light

TYPICAL APPLICATION CIRCUIT

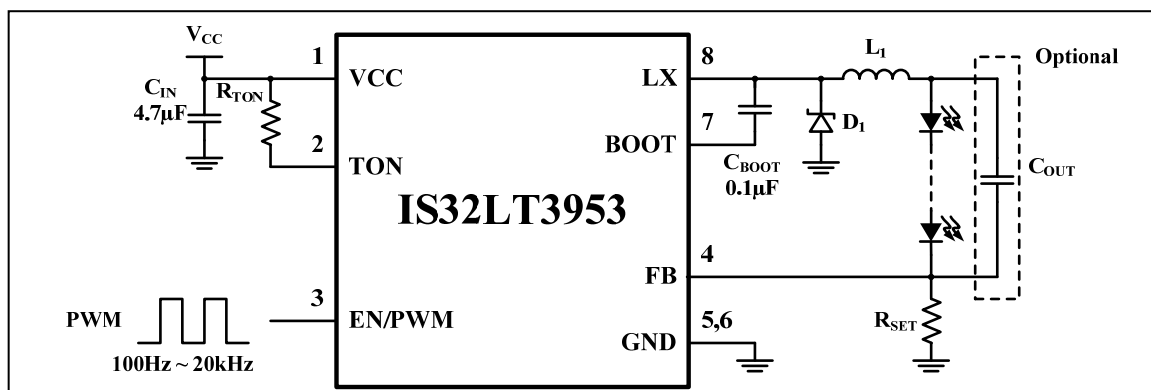
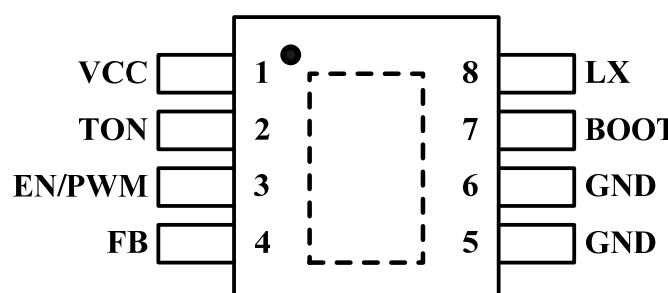


Figure 1 Typical Application Circuit

IS32LT3953

PIN CONFIGURATION

Package	Pin Configuration (Top View)
SOP-8-EP	 <p> VCC [] 1 [] 8 [] LX TON [] 2 [] 7 [] BOOT EN/PWM [] 3 [] 6 [] GND FB [] 4 [] 5 [] GND </p>

PIN DESCRIPTION

No.	Pin	Description
1	VCC	Power supply input. Connect a bypass capacitor C_{IN} to ground. The path from C_{IN} to GND and VCC pins should be as short as possible.
2	TON	On-time setting. Connect a resistor from this pin to VCC pin to set the regulator controlled on-time.
3	EN/PWM	Logic input for enable and PWM dimming. Pull up above 1.4V to enable and below 0.4V to disable. Input a 100Hz~20kHz PWM signal to dim the LED brightness.
4	FB	Drive output current sense feedback. Set the output current by connecting a resistor from this pin to the ground.
5, 6	GND	Ground.
7	BOOT	Internal MOSFET gate driver bootstrap. Connect a 0.1 μ F X7R ceramic capacitor from this pin to LX pin.
8	LX	Internal high-side MOSFET switch output. Connect this pin to the inductor and Schottky diode.
	Thermal Pad	Connect to GND.



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ORDERING INFORMATION

Automotive Range: -40°C to +125°C

Order Part No.	Package	QTY/Reel
IS32LT3953-GRLA3-TR	SOP-8-EP, Lead-free	2500

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ABSOLUTE MAXIMUM RATINGS

Input voltage, V_{CC}	-0.3V ~ +44V
Bootstrap drive voltage, V_{BOOT}	-0.3V ~ $V_{CC} + 6V$
Switching voltage, V_{LX}	-1.5V ~ $V_{CC} + 0.3V$
EN/PWM and TON voltage, $V_{EN/PWM}$, and V_{TON}	-0.3V ~ $V_{CC} + 0.3$
Current sense voltage, V_{FB}	-0.3V ~ 6.0V
Power dissipation, $P_{D(MAX)}$	2.29W
Operating temperature, $T_A = T_J$	-40°C ~ +125°C
Storage temperature, T_{ST}	-65°C ~ +150°C
Junction temperature, T_{JMAX}	+150°C
Junction Package thermal resistance, junction to ambient (4 layer standard test PCB based on JEDEC standard), θ_{JA}	43.7°C/W
Package thermal resistance, junction to thermal PAD (4 layer standard test PCB based on JEDEC standard), θ_{JP}	1.41°C/W
ESD (HBM)	±2kV
ESD (CDM)	±1kV

Note:

Stresses beyond those listed under “Absolute Maximum Ratings” may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other condition beyond those indicated in the operational sections of the specifications is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

ELECTRICAL CHARACTERISTICS

$V_{CC} = 24V$, $T_J = T_A = -40^\circ C \sim +125^\circ C$, Typical values are at $T_J = 25^\circ C$.

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
V_{CC}	Input supply voltage		4.5		40	V
V_{UVLO}	VCC undervoltage lockout threshold	V_{CC} increasing		4.3		V
V_{UVLO_HY}	VCC undervoltage lockout hysteresis	V_{CC} decreasing		250		mV
I_{CC}	VCC pin supply current	$V_{FB} = 0.5V$, $V_{EN/PWM} = \text{high}$		1.2		mA
I_{SD}	VCC pin shutdown current	EN/PWM shorted to GND		2	10	μA
I_{SWLIM}	Buck switch current limit threshold		3.5	4.5	5.5	A
t_{OCP}	Over Current Protection (OCP) hiccup time	(Note 1)		1		ms
R_{DS_ON}	Buck switch on-resistance	$V_{BOOT} = V_{CC} + 4.3V$, $T_J = 25^\circ C$, $I_{LX} = 1A$		0.25	0.4	Ω
V_{BTUV}	BOOT undervoltage lockout threshold	V_{BOOT} to V_{LX} increasing		3.3		V
V_{BTUV_HY}	BOOT undervoltage lockout hysteresis	V_{BOOT} to V_{LX} decreasing		400		mV
t_{OFF_MIN}	Switching minimum off-time	$V_{FB} = 0V$		120	150	ns
t_{ON_MIN}	Switching minimum on-time			110	150	ns
t_{ON}	Selected on-time	$V_{CC} = 24V$, $V_{OUT} = 12V$, $R_{TON} = 420k\Omega$	800	1000	1200	ns
Regulation Comparator and Error Amplifier						
V_{FB}	Load current sense regulation threshold	V_{FB} decreasing, LX turns on	190	200	210	mV
FAULT DETECTION						
t_{DELAY1}	Fault detect delay time			10		ms
t_{DELAY2}	Fault recover delay time			10		ms

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ELECTRICAL CHARACTERISTICS (CONTINUE)

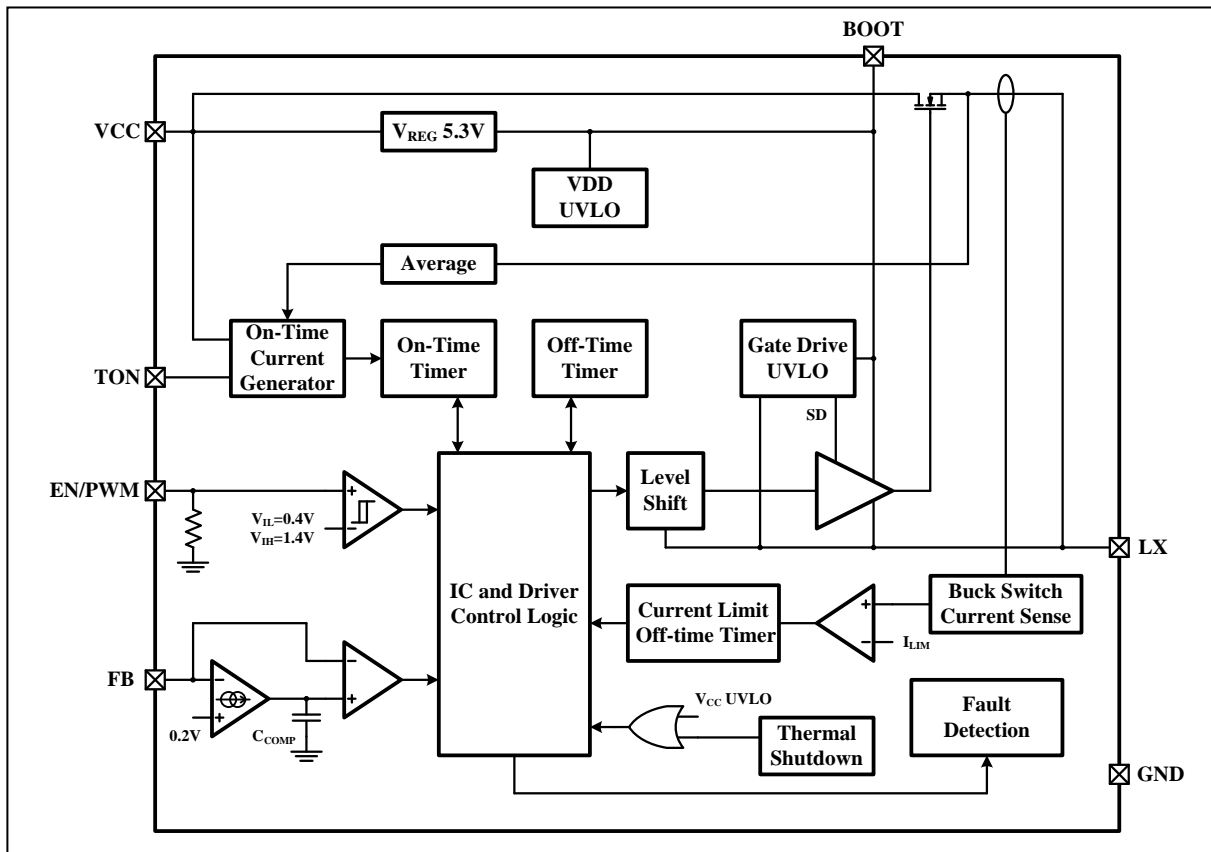
$V_{CC} = 24V$, $T_A = T_J = -40^{\circ}C \sim +125^{\circ}C$, Typical values are at $T_A = 25^{\circ}C$.

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
Enable Input						
V_{IH}	Logic high voltage	$V_{EN/PWM}$ increasing	1.4			V
V_{IL}	Logic low voltage	$V_{EN/PWM}$ decreasing			0.4	V
R_{PWMPD}	EN pin pull-down resistance	$V_{EN/PWM} = 5V$	150	200	250	k Ω
t_{PWML}	The time of EN/PWM pin keeping low to shutdown the device		55	65		ms
Thermal Shutdown						
T_{SD}	Thermal shutdown threshold	(Note 1)		165		$^{\circ}C$
T_{SDHYS}	Thermal shutdown hysteresis	(Note 1)		25		$^{\circ}C$

Note 1: Guaranteed by design.

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FUNCTIONAL BLOCK DIAGRAM



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APPLICATION INFORMATION

DESCRIPTION

The IS32LT3953 is a buck regulator with wide input voltage, low reference voltage, quick output response and excellent PWM dimming performance, which is ideal for driving a high-current LED string. It uses average current mode control to maintain constant LED current and consistent brightness.

UNDER VOLTAGE LOCKOUT (UVLO)

The device features the under voltage lockout (UVLO) function on VCC pin. It's internally fixed value and cannot be adjusted. The device is enabled when the VCC voltage rises to exceed V_{UVLO} (Typ. 4.3V), and disabled when the VCC voltage falls below $(V_{UVLO} - V_{UVLO_HY})$ (Typ. 4.1V).

BOOTSTRAP CIRCUIT

The gate driver of the integrated high-side MOSFET requires a voltage above VCC as power supply. As below circuit diagram, there is an internal 5.3V LDO which is the power supply of the gate driver. The BOOT pin is internally connected to the output of the 5.3V LDO. Connect a ceramic capacitor between BOOT and SW pins. The VCC supplies the power to the 5.3V LDO which charges the C_{BOOT} capacitor during high-side MOSFET off cycles. Then in high-side MOSFET on cycles, the C_{BOOT} hold the charge and boosts the BOOT pin to 5.3V higher than LX pin.

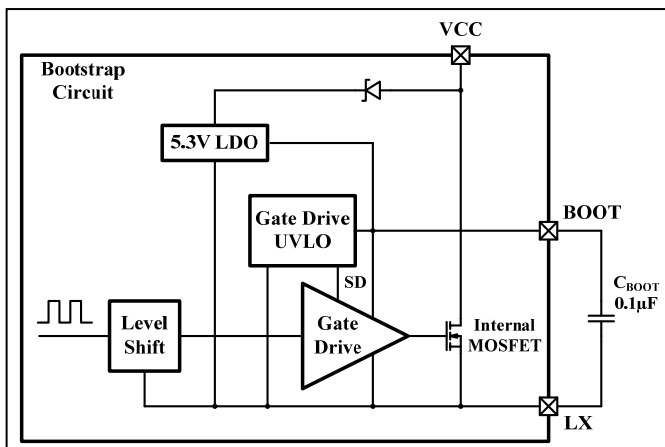


Figure 2 Bootstrap Circuit

A 0.1µF X7R ceramic capacitor will work well in most application. The gate driver also has a under voltage lockout detection. The gate driver is enabled when the voltage on the C_{BOOT} rises to above V_{BTUV} (Typ. 3.3V), and disabled when the voltage on the C_{BOOT} drops below $(V_{BTUV} - V_{BTUV_HY})$ (Typ. 2.9V).

OUTPUT CURRENT SETTING

The LED current is configured by an external sense resistor, R_{SET} , with a value determined as follows Equation (1):

$$I_{LED} = V_{FB} / R_{SET} \quad (1)$$

Where $V_{FB} = 0.2V$ (Typ.).

Note that $R_{SET} = 0.0667\Omega$ is the minimum allowed value of sense resistor to maintain switch current below the specified maximum value.

Table 1 R_{SET} Resistance Versus Output Current

R_{SET} (Ω)	Nominal Average Output Current (mA)
0.2	1000
0.1	2000
0.0667	3000

The R_{SET} should be a 1% resistor with enough power tolerance and good temperature characteristic to ensure accurate and stable output current.

ENABLE AND PWM DIMMING

A high logic signal on the EN/PWM pin will enable the IC. The buck converter ramps up the LED current to a target level which is set by external resistor, R_{SET} .

When pull the EN/PWM pin from high to low, the buck converter will turn off, but the IC remains in standby mode for up to t_{PWML} . If release the EN/PWM pin to high again within this period, the LED current will turn on immediately. Sending a PWM (pulse-width modulation) signal to the EN/PWM pin will active dimming of the LED. The resulting LED brightness is proportional to the duty cycle (t_{ON} / T) of the PWM signal. A practical range for PWM dimming frequency is between 100Hz and 20kHz.

There is an inherence PWM turn on delay time during continuous PWM dimming, about 1µs. A high frequency PWM signal has shorter period time that will degrade the PWM dimming linearity and the lowest dimming current. Therefore, a low frequency PWM signal is good for achieving better dimming contrast ratio. At a 200Hz PWM frequency, the dimming duty cycle can be varied from 100% down to 1% or lower.

If EN/PWM pin keeps low at least t_{PWML} , the IC enters shutdown mode to reduce power consumption. The next high signal on EN/PWM will initialize a full startup sequence, which includes a startup delay of approximately 130µs. This startup delay does not exist in the PWM operation.

The EN/PWM pin is high-voltage tolerant and can be directly connected to a power supply. However, a series resistor (10kΩ) is required to limit the current flowing into the EN pin if PWM is higher than the V_{CC} voltage at any time. If PWM is driven from a logic input, this series resistor is not necessary.

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INPUT CAPACITOR

The input capacitor provides the transient pulse current, which is approximately equal to I_{LED} , to the inductor of the converter when high-side MOSFET is on. X7R type ceramic capacitor is good choice for the input bypass capacitor to handle the ripple current since it has a very low equivalent series resistance (ESR) and low equivalent series inductance (ESL) capacitor. Use the following equation to estimate the approximate capacitance:

$$C_{IN_MIN} = \frac{I_{LED} \times t_{ON}}{\Delta V_{CC}} \quad (2)$$

Where, ΔV_{CC} is the acceptable input voltage ripple, generally choose 5%-10% of input voltage. t_{ON} is on-time of the high-side MOSFET in μs . A minimum input capacitance of $2X C_{IN_MIN}$ is recommended for most application.

OUTPUT CAPACITOR

IS32LT3953 control loop can accept the voltage ripple on FB that means it can operate without the output capacitor to save cost. On the contrary, the FB pin needs a certain amount of voltage ripple to keep control loop stability. So if it needs a capacitor on the output to reduce the LED current ripple while keep the same average current in some application cases, the capacitor must be added across the LED string exclude the FB resistor. The reduction of the LED current ripple by the capacitor depends on several factors: capacitor value, inductor current ripple, operating frequency, output voltage and so on. A several μF capacitor is sufficient for most applications. However, the output capacitor brings in more delay time of LED current during PWM dimming that will degrade the dimming contrast.

The output capacitor is used to filter the LED current ripple to an acceptable level. The equivalent series resistance (ESR), equivalent series inductance (ESL) and capacitance of the capacitor contribute to the output current ripple. Therefore, a low-ESR X7R type capacitor could be used.

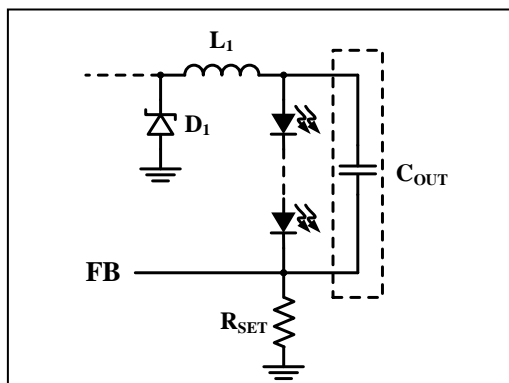


Figure 3 Adding Output Capacitor

FREQUENCY SELECTION

During switching the IS32LT3953 operates in a consistent on-time mode. The on-time is adjusted by an external resistor, R_{TON} , which is connected between the VCC and TON pins.

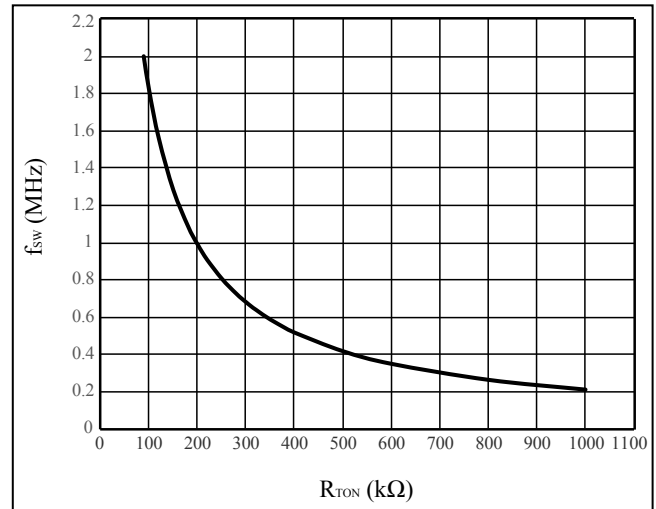


Figure 4 Operating Frequency vs. R_{TON} Resistance

The approximate operating frequency can be calculated by below Equation (2) and (3):

$$t_{ON} = \frac{k \times (R_{TON} + R_{INT}) \times V_{OUT}}{V_{CC}} \quad (3)$$

$$f_{sw} = \frac{1}{k \times (R_{TON} + R_{INT})} \quad (4)$$

Where $k = 0.00458$, with f_{sw} in MHz, t_{ON} in μs , and R_{TON} and R_{INT} (internal resistance, 20k Ω) in k Ω .

Higher frequency gets smaller components size but increases the switching losses and high-side MOSFET gate driving current, and may not allow sufficiently high or low duty cycle. Lower frequency gives better performance at larger components size.

SPREAD SPECTRUM

A switch mode controller can be particularly troublesome for application when the EMI is concerned. To optimize the EMI performance, the IS32LT3953 includes a spread spectrum feature, which is a 500Hz and $\pm 10\%$ operating frequency jitter. The spread spectrum can spread the total electromagnetic emitting energy into a wider range that significantly degrades the peak energy of EMI. With the spread spectrum, the EMI test can be easy to be passed with smaller size and lower cost filter circuit.

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MINIMUM AND MAXIMUM OUTPUT VOLTAGE

The output voltage of a buck converter is approximately given as below:

$$V_{OUT} = V_{CC} \times D \quad (5)$$

Where D is the operating duty cycle.

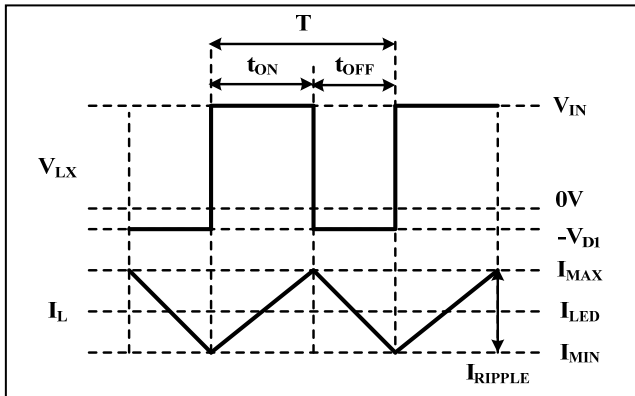


Figure 5 Operating Waveform

$$D = \frac{t_{ON}}{t_{ON} + t_{OFF}} \quad (6)$$

$$\text{So, } V_{OUT} = V_{CC} \times \frac{t_{ON}}{t_{ON} + t_{OFF}} = V_{CC} \times t_{ON} \times f_{SW} \quad (7)$$

Where t_{ON} and t_{OFF} are the turn-on and turn off time of high-side MOSFET. Note that due to the spread spectrum, the f_{SW} should use the maximum of the operating frequency, $120\% \times f_{SW}$.

According to above equation, the output voltage depends on the operating frequency and the high-side MOSFET turn on time. When the frequency is set, the maximum output voltage is limited by the switching minimum off-time t_{OFF_MIN} , about 150ns. For example, if the input voltage is 12V and the operating frequency $f_{SW}=1\text{MHz}$, the maximum output voltage is:

$$V_{OUT} = 12V \times (1\mu s - 150ns) \times 1MHz = 10.2V \quad (8)$$

Assume the forward voltage of each LED is 3.2V, the device can drive up to 3 LEDs in series.

By analogy, the minimum output voltage is limited by the switching minimum on-time, about 150ns, as the frequency is set. For example, if the input voltage is 12V and the operating frequency $f_{SW}=1\text{MHz}$, the minimum output voltage is:

$$V_{OUT} = 12V \times 150ns \times 1MHz = 1.8V \quad (9)$$

That means the device can drive a low forward voltage LED, such as a RED color LED. So under the condition of $V_{CC}=12V$ and $f_{SW}=1\text{MHz}$, the output voltage range is 1.8V~10.2V. Exceeding this range, the operating will be clamped and the output current cannot reach the set value.

In the real application, the output voltage is also slightly affected by some other affects, such as the output current, the R_{DS_ON} of the high-side MOSFET, the DCR of the inductor, the parasitic resistance of the PCB traces, and the forward voltage of the diode, so the output voltage range could be a little bit narrow than the calculation. The more precision equation is given by:

$$V_{OUT} = (V_{CC} - I_{LED} \times R_{DS_ON}) \times D - R_L \times I_{LED} - V_D \times (1 - D) \quad (10)$$

Where, R_{DS_ON} is static drain-source on resistance of high-side MOSFET, R_L is the inductor DC resistance.

Figure 6 shows how the minimum and maximum output voltages vary with the operating frequency at 12V and 24V input. Figure 7 shows how the minimum and maximum output voltages vary with the LED current at 9V input (assuming $R_{DS_ON} = 0.4\Omega$, inductor DCR $R_L = 0.1\Omega$, and diode $V_D = 0.6V$). Note that due to the spread spectrum, the f_{SW} should use the maximum of the operating frequency, $120\% \times f_{SW}$.

When the output voltage is lower than the minimum t_{ON} time of the device, the device will automatically extend the operating t_{OFF} time to maintain the set output LED current all the time. However, the operating frequency will decrease accordingly to lower level to keep the duty cycle in correct regulating.

To achieve wider output voltage range and flexible output configuration, a lower operating frequency could be considered.

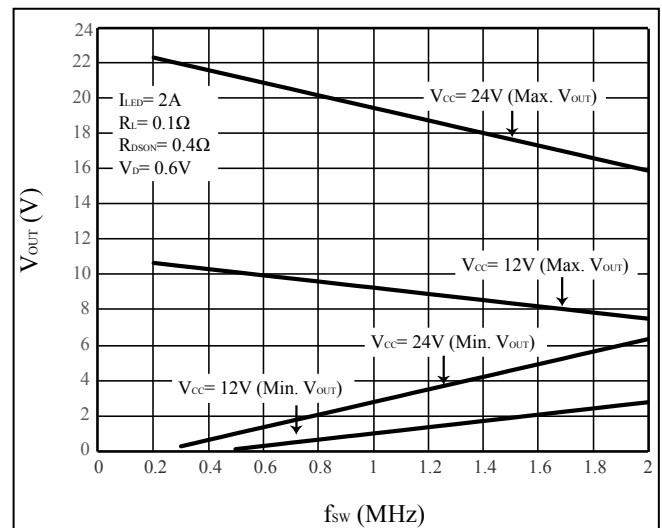


Figure 6 Minimum and Maximum Output Voltage versus Operating Frequency (minimum t_{ON} and $t_{OFF} = 150ns$)

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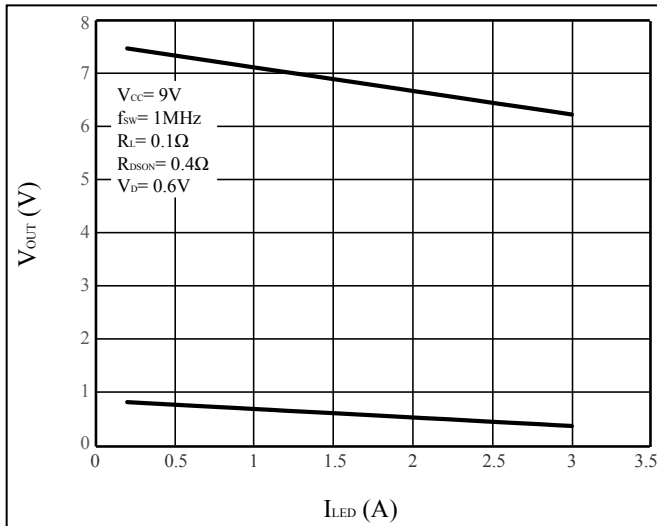


Figure 7 Minimum and Maximum Output Voltage versus LED Current (minimum t_{ON} and t_{OFF} = 150ns)

PEAK CURRENT LIMIT

To protect the device, IS32LT3953 integrates an Over Current Protection (OCP) detection circuit to monitor the current through the high-side MOSFET during switching on. Whenever the current exceeds OCP current threshold, I_{SWLIM} , the device will immediately turn off the high-side MOSFET for t_{OCP} and restart again. The device will keep in this kind hiccup mode until the current drops below I_{SWLIM} .

INDUCTOR

Inductor value involves trade-offs in performance. Larger inductance reduces inductor current ripple that obtains smaller output current ripple, however it also brings in unwanted parasitic resistance that degrade the performance. Smaller inductance has compact size and lower cost, but introduces higher ripple in the LED string. Use the following equations to estimate the approximate inductor value:

$$L = \frac{(V_{CC} - V_{LED}) \times V_{LED}}{f_{SW} \times \Delta I_L \times V_{CC}} \quad (11)$$

Where V_{CC} uses the minimum input voltage in volts, V_{LED} is the total forward voltage of LED string in volts, f_{SW} is the operation frequency in hertz. ΔI_L is the current ripple in the inductor. Select an inductor with a rating current over output average current and the saturation current over the Over Current Protection (OCP) current threshold I_{SWLIM} .

Since IS32LT3953 is a Continuous Conduction Mode (CCM) buck driver which means the valley of the inductor current, I_{MIN} , should not drop to zero all the time, the ΔI_L must be smaller than 200% of the average output current.

$$I_{MIN} = I_{LED} - \frac{\Delta I_L}{2} > 0 \quad (12)$$

Besides, the peak current of the inductor, I_{MAX} , must be

smaller than I_{SWLIM} to prevent device from triggering OCP, especially the output current is set to high level.

$$I_{MAX} = I_{LED} + \frac{\Delta I_L}{2} < I_{SWLIM} \quad (13)$$

On the other hand, the ΔI_L has to be higher than 10% of the average output current all the time to ensure the system stability. For the better performance, recommend to choose the inductor current ripple ΔI_L between 10% and 50% of the average output current.

$$0.1 \times I_{LED} \leq \Delta I_L \leq 0.5 \times I_{LED} \quad (14)$$

Below figure shows the inductance selection based on operating frequency and LED current at 30% inductor current ripple. If the lower operating frequency is adopted, either the larger inductance or current ripple should be used.

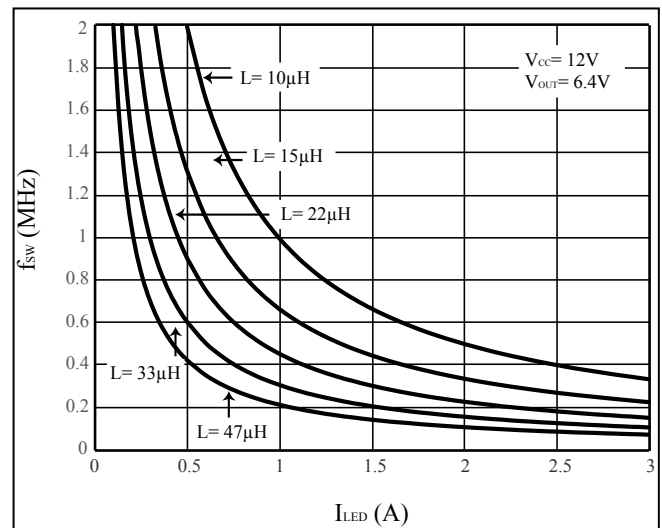


Figure 8 Inductance Selection Based On 30% Current Ripple

DIODE

IS32LT3953 is non-synchronous buck driver that requires a recirculating diode to conduct the current during the high-side MOSFET off time. The best choice is a Schottky diode due to its low forward voltage, low reverse leakage current and fast reverse recovery time. The diode should be selected with a peak current rating above the inductor peak current and a continuous current rating higher than the maximum output load current. It is very important to consider the reverse leakage of the diode when operating at high temperature. Excess leakage will increase the power dissipation on the device.

The higher input voltage and the voltage ringing due to the reverse recovery time of the Schottky diode will increase the peak voltage on the LX output. If a Schottky diode is chosen, care should be taken to ensure that the total voltage appearing on the LX pin including supply ripple, does not exceed its specified maximum value.

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THERMAL SHUTDOWN PROTECTION

To protect the IC from damage due to high power dissipation, the temperature of the die is monitored. If the die temperature exceeds the thermal shutdown temperature of 165°C (Typ.) then the device will shut down, and the output current are shut off. After a thermal shutdown event, the IS32LT3953 will not try to restart until its temperature has reduced to less than 140°C (Typ.).

FAULT HANDLING

The IS32LT3953 is designed to detect the following faults:

- Pin open
- Pin-to-ground short
- Pin-to-neighboring pin short
- Output LED string open and short
- External component open or short

Please check Table 2 for the detail of the fault actions.

Table 2 Fault Actions

Fault Type	LED String	Detect Condition		Fault Recovering
Inductor shorted	Dim	Trigger OCP. Turn off high-side MOSFET immediately. Retry after 1ms.		Inductor shorted removed. No OCP triggered.
R _{SET} short	Dim	Trigger OCP. Turn off high-side MOSFET immediately. Retry after 1ms.		R _{SET} shorted removed. No OCP triggered.
R _{SET} open	Off	The FB pin voltage exceed 2V. Turn off high-side MOSFET immediately. Retry after 1ms.		R _{SET} open removed. The FB pin voltage drops below 1.55V.
LED string open	Off	No PWM dimming:	FB pin average voltage drops below 0.2V for 10ms.	LED open removed. FB average voltage keep at 0.2V for 10ms.
		PWM dimming:	FB pin average voltage drops below 0.2V after 25us deglitch time and keeps for 128 PWM cycles.	
LED string shorted	Off	No PWM dimming:	Filter V _{LX} to get V _{OUT} , if V _{OUT} <1V for 10ms	Shorted removed. V _{OUT} >1V for 10ms.
		PWM dimming:	Filter V _{LX} to get V _{OUT} , if V _{OUT} <1V after 25us deglitch time and keeps for 128 PWM cycles.	
LED string shorted to GND	Off	Trigger OCP. Turn off high-side MOSFET immediately. Retry after 1ms.		Shorted removed. No OCP triggered.
BOOT capacitor open	Dim	VCC-V _{sw} >1.8V at high-side MOSFET ON (High-side can't fully turn on). Turn off high-side MOSFET immediately. Retry after 1ms.		BOOT capacitor open removed, VCC-V _{sw} <1.8V for 10ms.
BOOT capacitor shorted	Off	Bootstrap circuit UVLO and turn off high-side MOSFET immediately.		BOOT capacitor shorted removed. Release from UVLO.
R _{TON} resistor open	Dim	On-time exceeds 20us or trigger OCP, then turn off high-side MOSFET immediately. Retry after 1ms.		R _{TON} resistor open removed. No over 20us on-time or OCP triggered.
R _{TON} resistor shorted	Dim	The device operating at minimum on/off time, maybe trigger the other fault conditions.		R _{TON} resistor shorted removed.
EN short to R _{SET}	Off	EN/PWM will be pulled low by R _{SET} resistor.		EN short to R _{SET} removed.

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LAYOUT CONSIDERATIONS

As for all switching power supplies, especially those providing high current and using high switching frequencies, layout is an important design step. If layout is not carefully done, the operation could show instability as well as EMI problems.

The high dV/dt surface and dI/dt loops are big noise emission source. To optimize the EMI performance, keep the area size of all high switching frequency points with high voltage compact. Meantime, keep all traces carrying high current as short as possible to minimize the loops.

- (1) Wide traces should be used for connection of the high current paths that helps to achieve better efficiency and EMI performance. Such as the traces of power supply, inductor L₁, current recirculating diode D₁, LED load and ground.
- (2) Keep the traces of the switching points shorter. The inductor L₁, LX and current recirculating diode D₁ should be placed as close to each other as possible and the traces of connection between them should be as short and wide as possible.
- (3) To avoid the ground jitter, the components of parameter setting, R_{SET}, should be placed close to the device and keep the traces length to the device pins as short as possible. On the other side, to prevent the noise coupling, the traces of R_{SET} should either be far away or be isolated from high-current paths and high-speed switching nodes. These practices are essential for better accuracy and stability.
- (4) The capacitor C_{IN} should be placed as close as possible to VCC pin for good filtering.
- (5) Place the bootstrap capacitor C_{BOOT} close to BOOT pin and LX pin to ensure the traces as short as possible.
- (6) The connection to the LED string should be kept short to minimize radiated emission. In practice, if the LED string is far away from the driver board, an output capacitor is recommended to be used and placed on driver board to reduce the current ripple in the connecting wire.
- (7) The thermal pad on the back of device package must be soldered to a sufficient size of copper ground plane with sufficient vias to conduct the heat to opposite side PCB for adequate cooling.

THERMAL CONSIDERATIONS

The package thermal resistance, θ_{JA} , determines the amount of heat that can pass from the silicon die to the surrounding ambient environment. The θ_{JA} is a measure of the temperature rise created by power dissipation and is usually measured in degree Celsius per watt ($^{\circ}C/W$).

When operating the chip at high ambient temperatures, or when driving maximum load current, care must be taken to avoid exceeding the package power dissipation limits. The maximum power dissipation can be calculated using the following Equation (15):

$$P_{D(MAX)} = \frac{T_{J(MAX)} - T_A}{\theta_{JA}} \quad (15)$$

So,

$$P_{D(MAX)} = \frac{125^{\circ}C - 25^{\circ}C}{43.7^{\circ}C/W} \approx 2.29W$$

Figure 9, shows the power derating of the IS32LT3953 on a JEDEC boards (in accordance with JESD 51-5 and JESD 51-7) standing in still air.

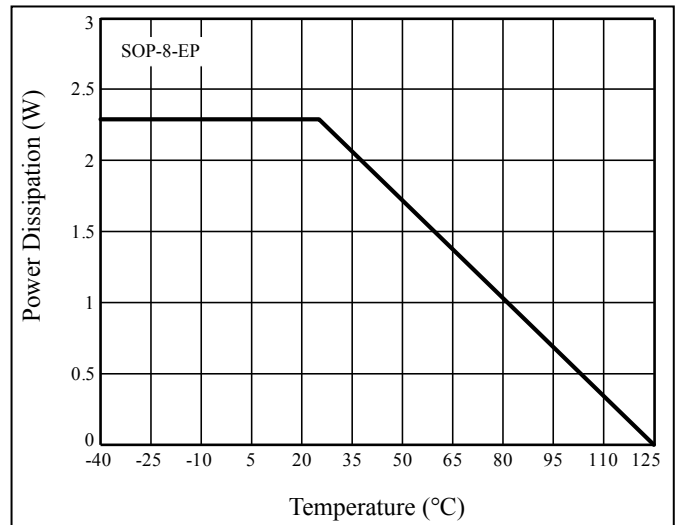


Figure 9 Dissipation Curve

The thermal resistance is achieved by mounting the IS32LT3953 on a standard FR4 double-sided printed circuit board (PCB) with a copper area of a few square inches on each side of the board under the IS32LT3953. Multiple thermal vias, as shown in Figure 10, help to conduct the heat from the exposed pad of the IS32LT3953 to the copper on each side of the board. The thermal resistance can be reduced by using a metal substrate or by adding a heatsink.

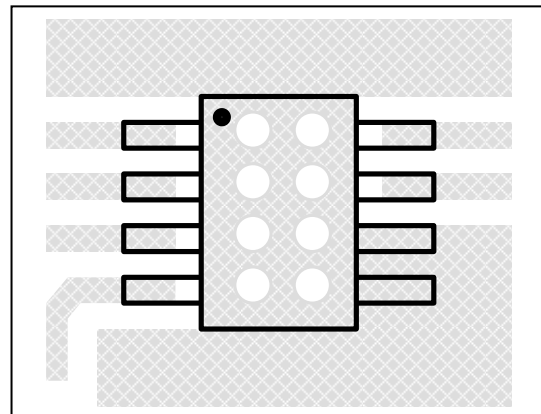


Figure 10 Board Via Layout For Thermal Dissipation

IS32LT3953

CLASSIFICATION REFLOW PROFILES

Profile Feature	Pb-Free Assembly
Preheat & Soak Temperature min (T _{smn}) Temperature max (T _{smax}) Time (T _{smn} to T _{smax}) (t _s)	150°C 200°C 60-120 seconds
Average ramp-up rate (T _{smax} to T _p)	3°C/second max.
Liquidous temperature (T _L) Time at liquidous (t _L)	217°C 60-150 seconds
Peak package body temperature (T _p)*	Max 260°C
Time (t _p)** within 5°C of the specified classification temperature (T _c)	Max 30 seconds
Average ramp-down rate (T _p to T _{smax})	6°C/second max.
Time 25°C to peak temperature	8 minutes max.

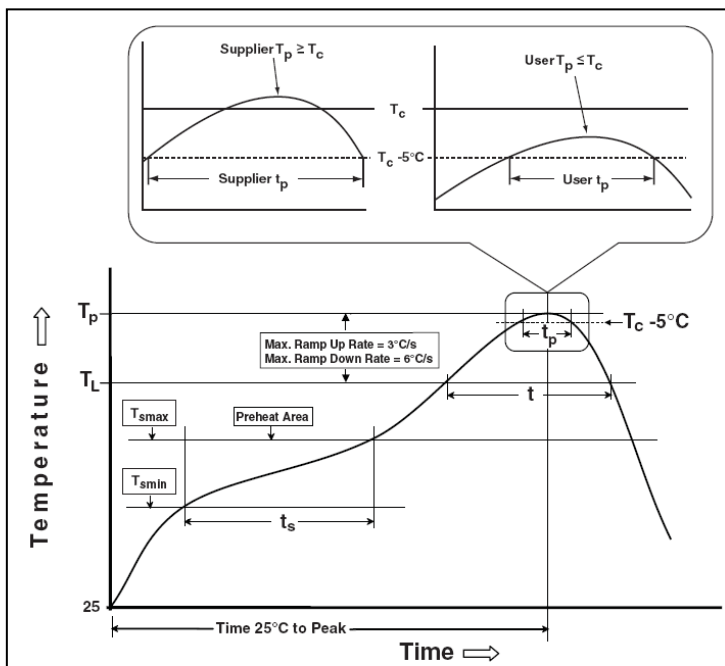
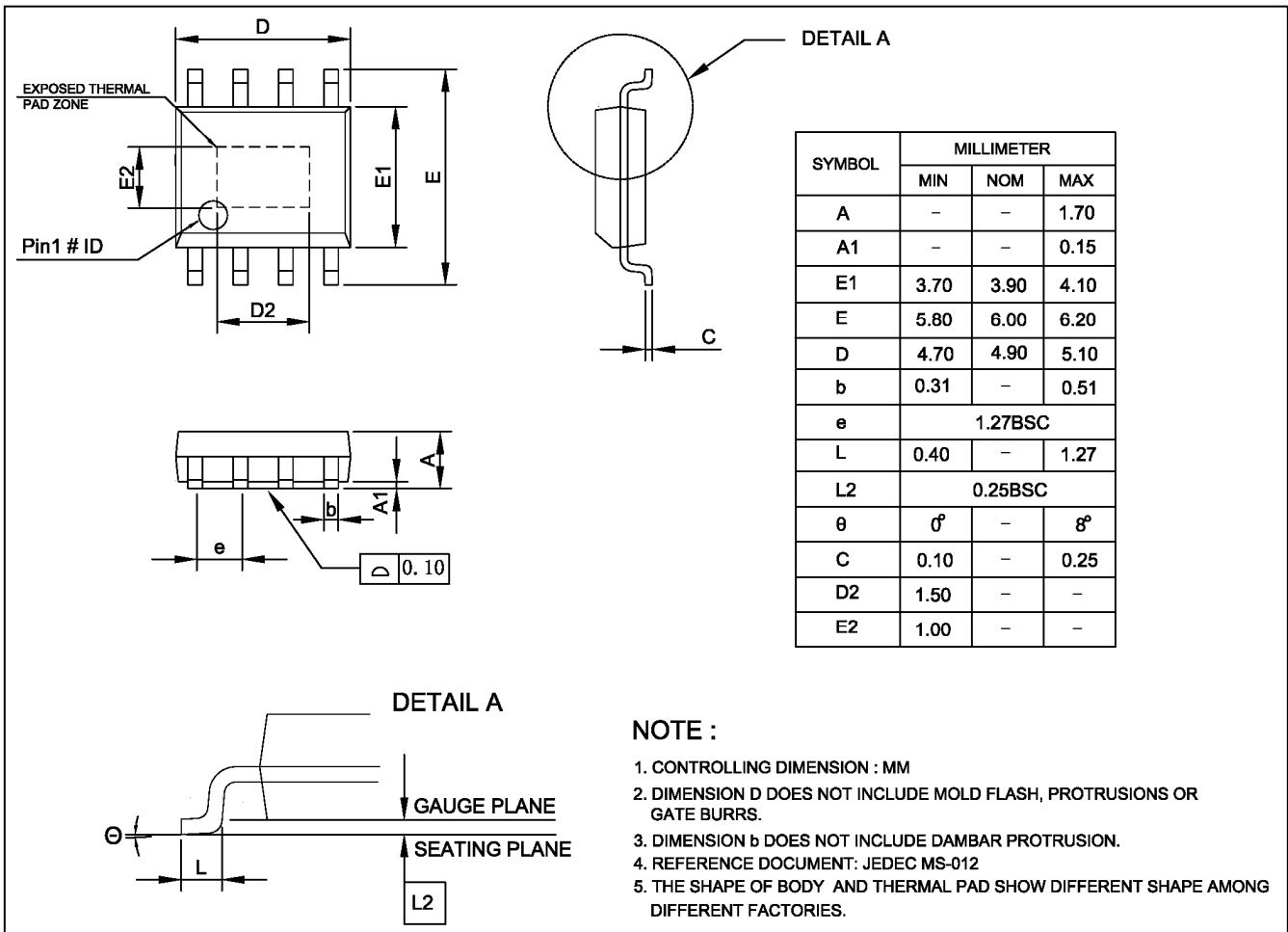


Figure 11 Classification Profile

IS32LT3953

PACKAGE INFORMATION

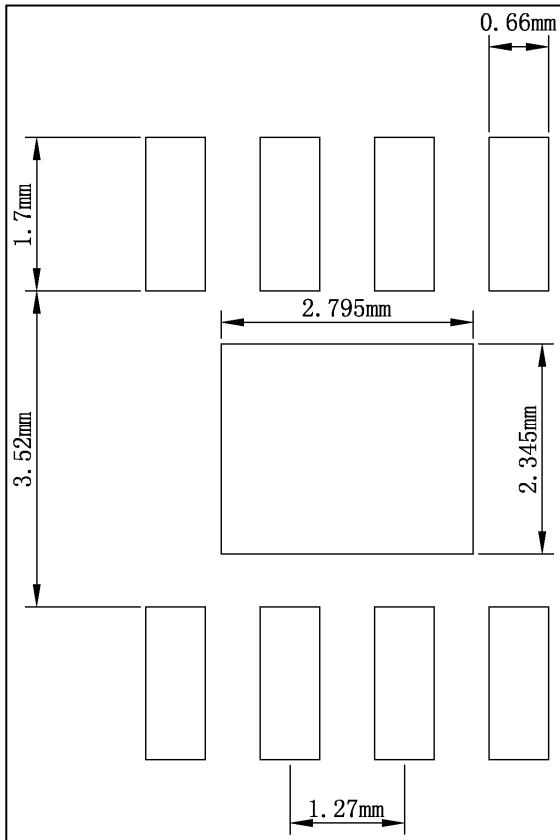
SOP-8-EP



IS32LT3953

RECOMMENDED LAND PATTERN

SOP-8-EP



Note:

1. Land pattern complies to IPC-7351.
2. All dimensions in MM.
3. This document (including dimensions, notes & specs) is a recommendation based on typical circuit board manufacturing parameters. Since land pattern design depends on many factors unknown (eg. user's board manufacturing specs), user must determine suitability for use.



IS32LT3953

REVISION HISTORY

Revision	Detail Information	Date
0A	Initial release	2017.04.10
0B	1. Update EC table and fault table 2. Update land pattern	2017.11.14